

# Ch6: Time Response

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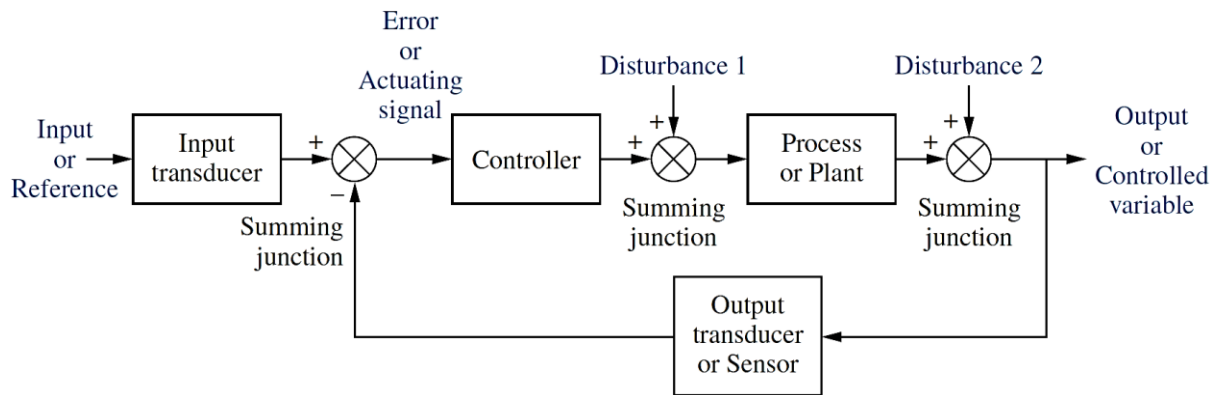
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# Introduction

# Introduction

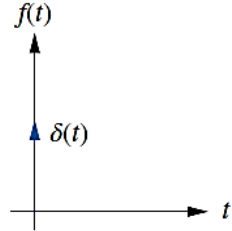
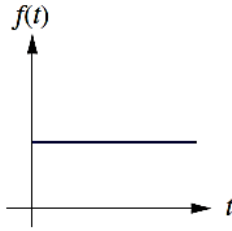
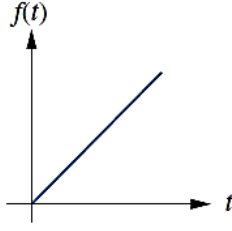
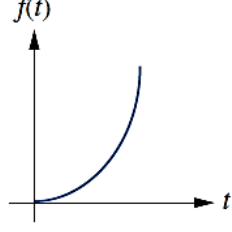
After obtaining a mathematical representation of a system, it is **analyzed** for its performance, i.e., **transient response**, **steady-state response**, and **stability**, to see if these characteristics yield the desired behavior.

- In practice, the input signal to a control system is not known ahead of time and is random in nature. Hence, in analysis and design of control systems, we must have a basis for comparing the performance of various control systems.
- This basis may be set up by specifying particular **test input signals** (that the system will be subjected to most frequently under normal operation) and comparing the responses of various systems (with zero initial condition) to these input signals.



# Typical Test Input Signals

The commonly used  
**test input signals:**  
impulse,  
step,  
ramp,  
parabola,  
sinusoidal,  
white noise.

Input	Function	Description	Sketch	Use
Impulse	$\delta(t)$	$\delta(t) = \infty$ for $0- < t < 0+$ $= 0$ elsewhere $\int_{0-}^{0+} \delta(t) dt = 1$		Transient response Modeling
Step	$u(t)$	$u(t) = 1$ for $t > 0$ $= 0$ for $t < 0$		Transient response Steady-state error
Ramp	$tu(t)$	$tu(t) = t$ for $t \geq 0$ $= 0$ elsewhere		Steady-state error
Parabola	$\frac{1}{2}t^2u(t)$	$\frac{1}{2}t^2u(t) = \frac{1}{2}t^2$ for $t \geq 0$ $= 0$ elsewhere		Steady-state error

# Order of a System

**Order** of a system is

- The order of the equivalent differential equation representing the system.

$$a_n \frac{d^n c(t)}{dt^n} + a_{n-1} \frac{d^{n-1} c(t)}{dt^{n-1}} + \dots + a_0 c(t) = b_m \frac{d^m r(t)}{dt^m} + b_{m-1} \frac{d^{m-1} r(t)}{dt^{m-1}} + \dots + b_0 r(t)$$

- The highest power of  $s$  in the denominator of the transfer function **after** cancellation of common factors in the numerator.

$$G(s) = \frac{b_m s^m + b_{m-1} s^{m-1} + \dots + b_0}{a_n s^n + a_{n-1} s^{n-1} + \dots + a_0} = \frac{(s + z_1)(s + z_2) \dots (s + z_m)}{(s + p_1)(s + p_2) \dots (s + p_n)}$$

- The number of simultaneous first-order equations required for the state-space representation of the system (i.e., the dimension of vector  $\mathbf{x}$  or the number of states).

$$\begin{aligned}\dot{\mathbf{x}}(t) &= \mathbf{A}\mathbf{x}(t) + \mathbf{B}\mathbf{u}(t) \\ \mathbf{y}(t) &= \mathbf{C}\mathbf{x}(t) + \mathbf{D}\mathbf{u}(t)\end{aligned}$$

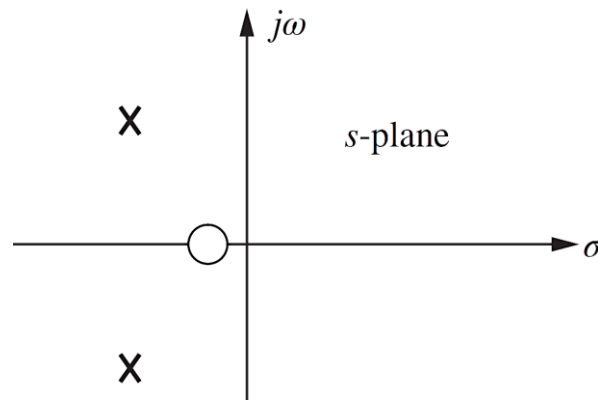
# Poles & Zeros of a Transfer Function

$$G(s) = \frac{b_m s^m + b_{m-1} s^{m-1} + \dots + b_0}{a_n s^n + a_{n-1} s^{n-1} + \dots + a_0} = \frac{(s + z_1)(s + z_2) \dots (s + z_m)}{(s + p_1)(s + p_2) \dots (s + p_n)}$$

**Poles of a Transfer Function ( $p_i$ )** are (1) the values of the Laplace transform variable,  $s$ , that cause the transfer function to become infinite or (2) any roots of the denominator of the transfer function that are common to roots of the numerator (i.e., before cancelation).

**Zeros of a Transfer Function ( $z_i$ )** are (1) the values of the Laplace transform variable,  $s$ , that cause the transfer function to become zero, or (2) any roots of the numerator of the transfer function that are common to roots of the denominator (i.e., before cancelation).

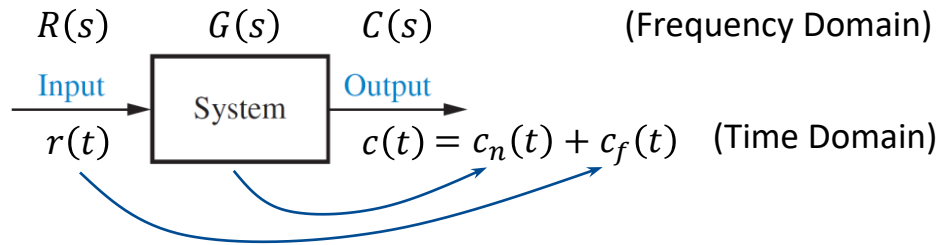
Symbol of **pole** on the complex  $s$ -plane: **x**  
Symbol of **zero** on the complex  $s$ -plane: **o**



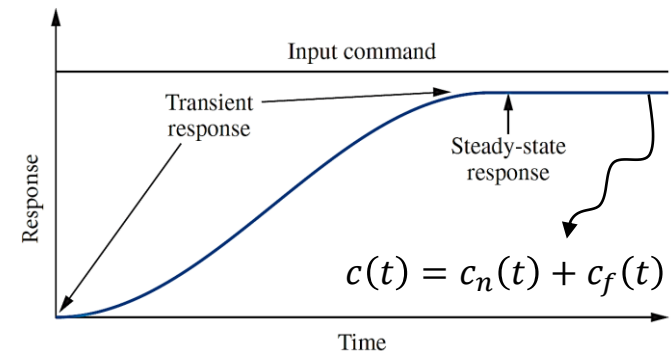
# Forced & Natural Responses vs Transient & Steady-State Responses

The total time response  $c(t)$  of a linear system is the sum of two responses:

- 1) **Natural Response** (or **homogeneous solution**)  $c_n(t)$  which depends only on the system, not the input.
- 2) **Forced Response** (or **particular solution**)  $c_f(t)$  which depends only on the input, not the system.

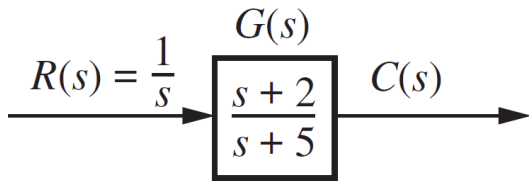


By considering the **response plot**, it is inferred that the response can consist of two parts, the **Transient** response (the way it goes from the initial state to the final state) and **Steady-State** response (the way it behaves as time approaches infinity).

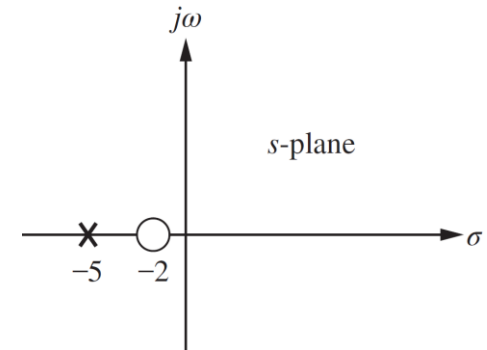


❖ **Natural Response** contributes more to the **Transient Response** and **Force Response** contributes more to the **Steady-State Response**.

# Example: Time Response of a System



Pole:  $s = -5$   
 Zero:  $s = -2$

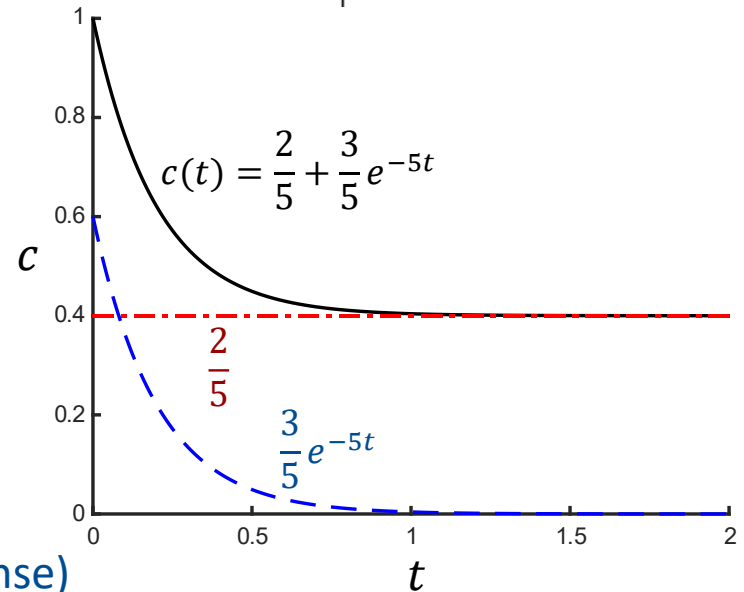


The unit step response of the system:

$$C(s) = \frac{(s+2)}{s(s+5)} = \frac{K_1}{s} + \frac{K_2}{s+5} = \frac{2/5}{s} + \frac{3/5}{s+5}$$

$$c(t) = \frac{2}{5} + \frac{3}{5}e^{-5t}$$

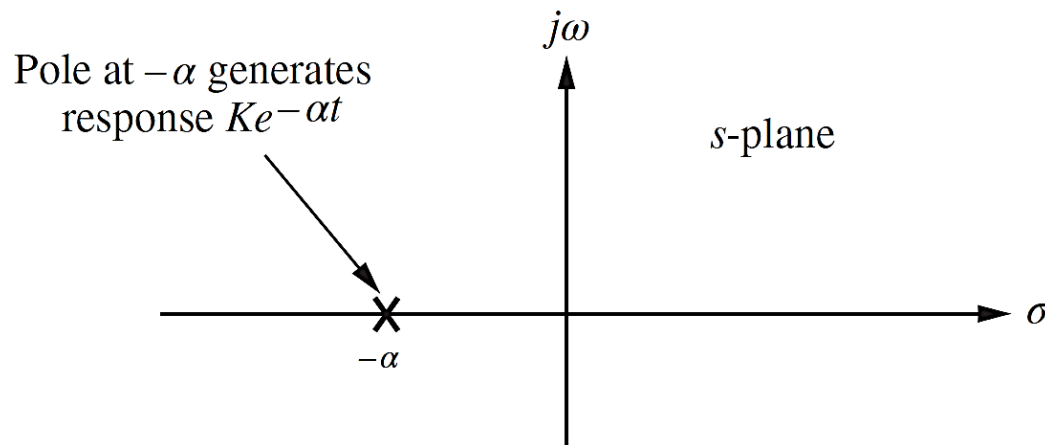
(Forced response)      (Natural response)





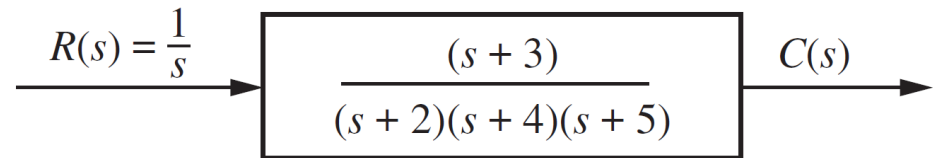
# Important Conclusions

- a. Poles of the transfer function determine the form of the **natural response** (exponential, sinusoid, ...),
- b. Poles of the input function determine the form of the **forced response**,
- c. Zeros and poles of the input and transfer function contribute to the amplitudes (or residues), i.e.,  $K_1$  and  $K_2$ , of both the forced and natural responses,
- d. Non-zero poles **on the real axis** ( $-\alpha$ ) generate **exponential** responses ( $e^{-\alpha t}$ ). Therefore, the farther to the left a pole is on the negative real axis, the faster the exponential transient response will decay to zero



# Example: Evaluating Response Using Poles

Specify the forced and natural parts of the solution.



**Answer:**

$$c(t) = \underbrace{K_1}_{\text{Forced response}} + \underbrace{K_2 e^{-2t} + K_3 e^{-4t} + K_4 e^{-5t}}_{\text{Natural response}}$$

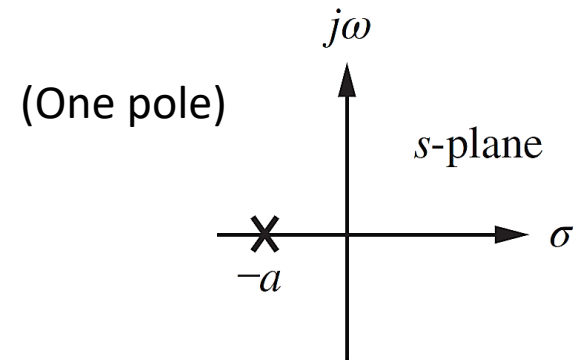
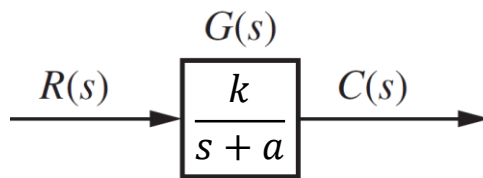
# First-Order Systems

# First-Order Systems

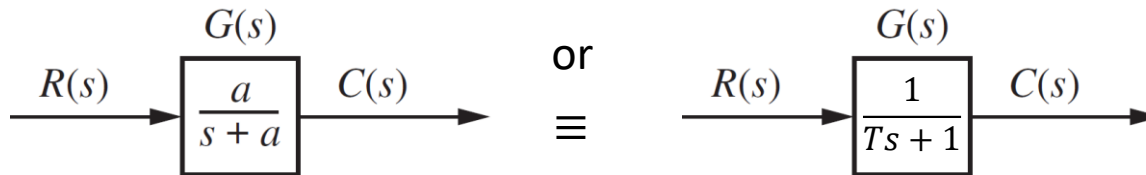
Consider a **First-Order System** (without zeros) with zero initial conditions.

[Physical Examples: RC circuit, thermal system]

- General Form:



- Standard Form (used to normalize response):



# Unit-Step Response

$$R(s) = 1/s$$

$$C(s) = R(s)G(s) = \frac{a}{s(s+a)} = \frac{1}{s} - \frac{1}{s+a}$$

$$c(t) = c_f(t) + c_n(t) = 1 - e^{-at}$$

$$= 1 - e^{-t/T}$$

$$c(\infty) = 1$$

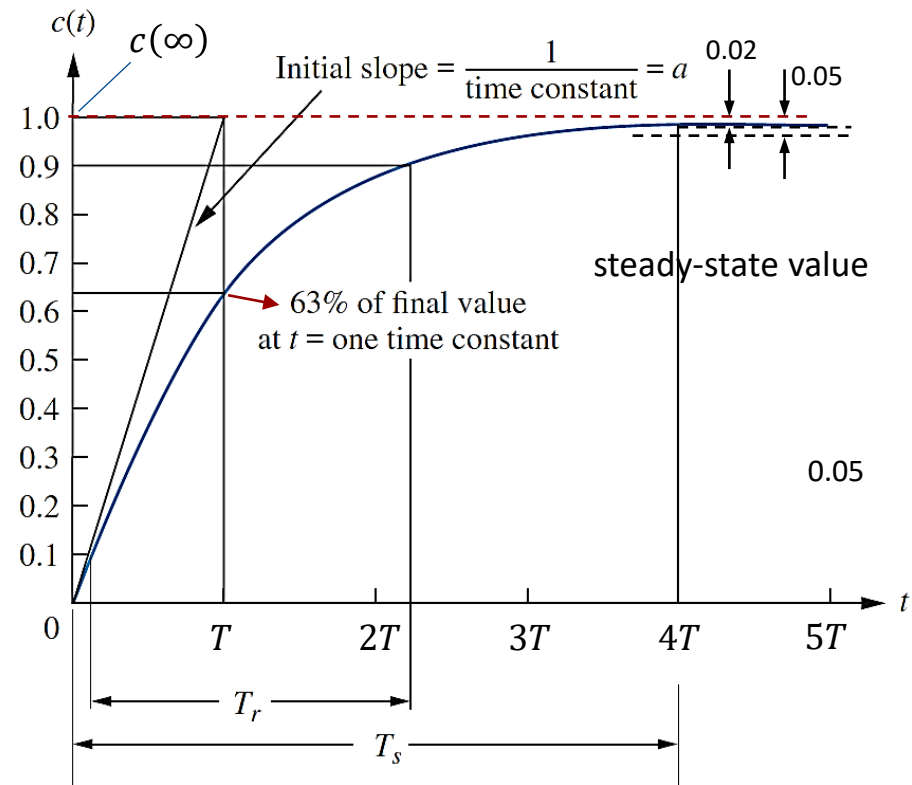
## Transient Response Specifications:

**1. Time Constant  $T$ :** The time required for the step response to rise to 63% of the steady-state value (final value).

$$T = t \Big|_{c(t)=0.63c(\infty)} = \frac{1}{a}$$

$$c(t) \Big|_{t=1/a} = 1 - e^{-1} \approx 0.63$$

• The initial rate of change (slope) of response is  $a$  or  $1/T$ .  $\frac{dc(t)}{dt} \Big|_{t=0} = a = \frac{1}{T}$



# Unit-Step Response

**2. Rise Time  $T_r$ :** The time required for the step response to go from 10% to 90% of the steady-state value.

$$T_r = t \Big|_{c(t)=0.9c(\infty)} - t \Big|_{c(t)=0.1c(\infty)} = \frac{-\ln(0.1)}{a} - \frac{-\ln(0.9)}{a} \approx \frac{2.30}{a} - \frac{0.10}{a} = \frac{2.2}{a}$$

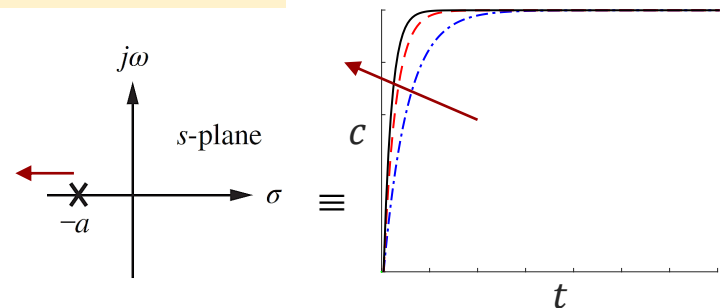
$$\Rightarrow T_r = \frac{2.2}{a} = 2.2T$$

**3. Settling Time  $T_s$ :** The time required for the step response to reach and stay within 2% (or 5%) of the steady-state value.

$$T_s = t \Big|_{c(t)=0.98c(\infty)} = \frac{-\ln(0.02)}{a} \approx \frac{4}{a} \Rightarrow$$

$$T_s = \frac{4}{a} = 4T$$

**Note:** The farther to the left the pole ( $-a$ ) from the imaginary axis  $j\omega$ , the faster the transient response.



# Example

For the given the transfer function. Find the time constant  $T$ , settling time  $T_s$ , and rise time  $T_r$ .

$$G(s) = \frac{100}{s + 50}$$

**Answer:**  $T = \frac{1}{a} = \frac{1}{50} = 0.02s$

$$T_s = \frac{4}{a} = \frac{4}{50} = 0.08s$$

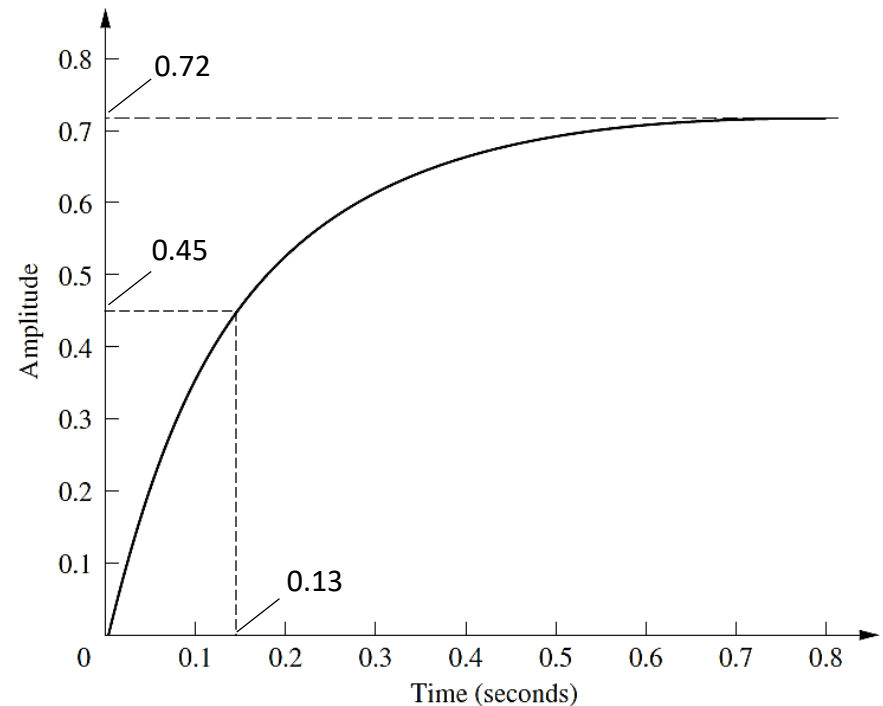
$$T_r = \frac{2.2}{a} = \frac{2.2}{50} = 0.044s$$

**Note:**  $T$ ,  $T_r$ , and  $T_s$  are independent of the value of  $k$  in the general form of a first order system  $\frac{k}{s+a}$ .

# Example: Determining Transfer Function via Testing

Often it is not possible or practical to obtain a system's transfer function analytically. Therefore, the system's step response can lead to a representation of the system.

The unit-step response of an unknown system is given. Determine its transfer function.



**Answer:**

$$G(s) = \frac{5.54}{s + 7.7}$$



# Unit-Ramp Response

$$R(s) = 1/s^2$$

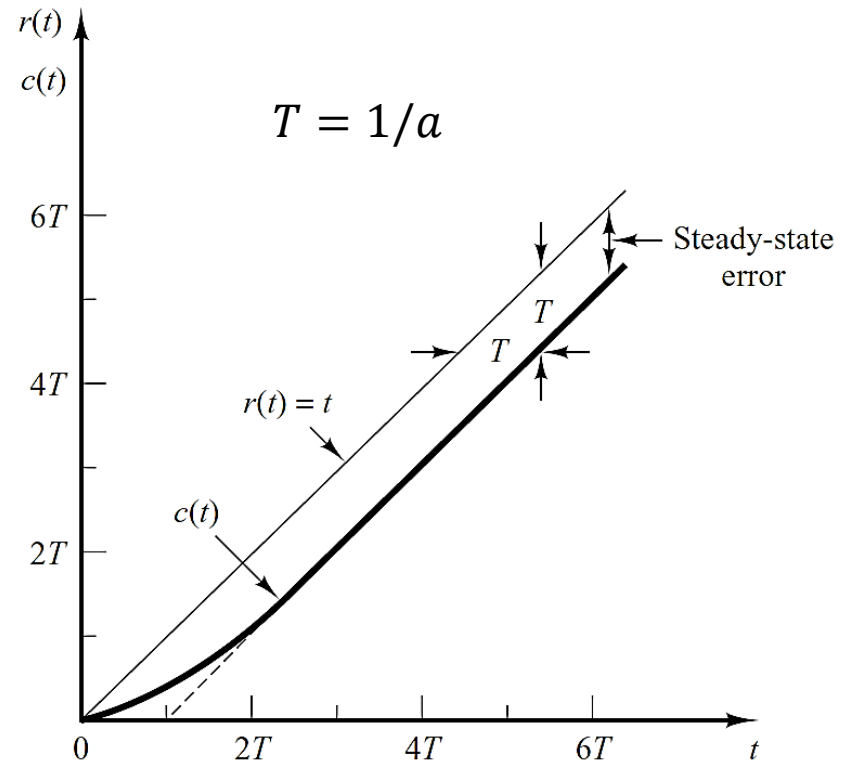
$$C(s) = R(s)G(s) = \frac{a}{s^2(s+a)}$$

$$= \frac{1}{s^2} - \frac{1/a}{s} + \frac{1/a}{s+a}$$

$$c(t) = c_f(t) + c_n(t) = t - \frac{1}{a} + \frac{1}{a}e^{-at}$$

$$e(t) = r(t) - c(t) = \frac{1}{a}(1 - e^{-at})$$

$$\lim_{t \rightarrow \infty} e(t) = \frac{1}{a} = T$$



**Note:** The farther to the left the pole ( $-a$ ) from the imaginary axis  $j\omega$ , the smaller the steady-state error in following the ramp input.

# Unit-Impulse Response

$$R(s) = 1$$

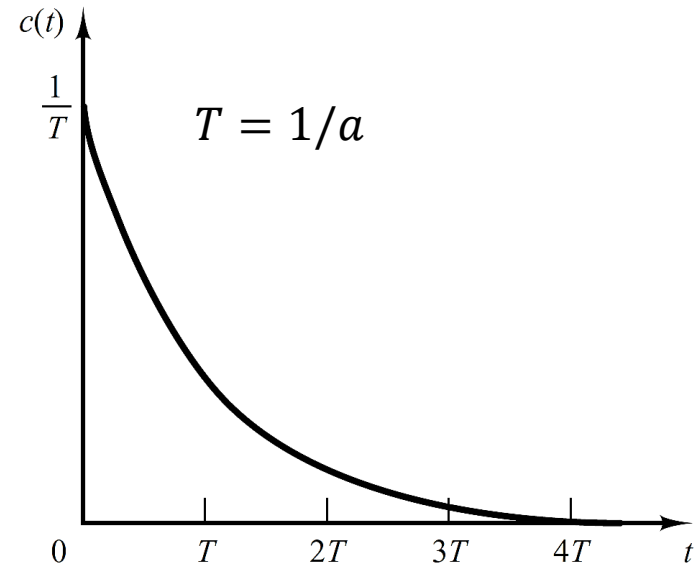
$$C(s) = R(s)G(s) = \frac{a}{s + a}$$

$$c(t) = \cancel{c_f(t)} + c_n(t) = ae^{-at}$$

0 ↙

**Note:**

$$\begin{array}{l} T\dot{x} + x = \delta(t), \\ x(0^-) = 0 \end{array} \iff \begin{array}{l} T\dot{w} + w = 0, \\ w(0^+) = 1/T \end{array}$$



## An Important Property of LTI Systems:

Comparing the system responses to these three inputs clearly indicates that the response to the **derivative/integral** of an input signal  $r$  can be obtained by **differentiating/integrating** the response  $c$  of the system to the original input signal  $r$ .

$$\begin{array}{l} r \rightarrow c \\ dr/dt \rightarrow dc/dt \\ \int r \rightarrow \int c \end{array}$$

$$r_{\text{impulse}} \xLeftrightarrow{d/dt} r_{\text{step}} \xLeftrightarrow{d/dt} r_{\text{ramp}} \implies c_{\text{impulse}} \xLeftrightarrow{d/dt} c_{\text{step}} \xLeftrightarrow{d/dt} c_{\text{ramp}}$$

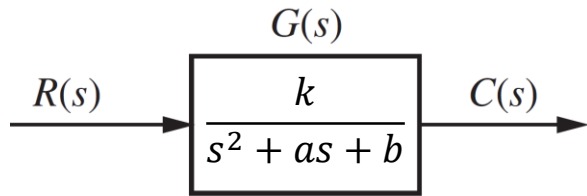
# Second-Order Systems

# Second-Order Systems

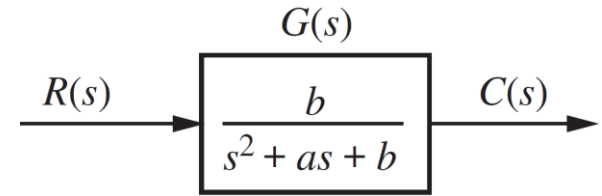
Consider a **Second-Order System** (without zeros) with zero initial conditions.

[Physical Examples: RLC circuit, Mass-Spring-Damper System, DC Motor]

- General Form:



- Standard Form (used to normalize response):

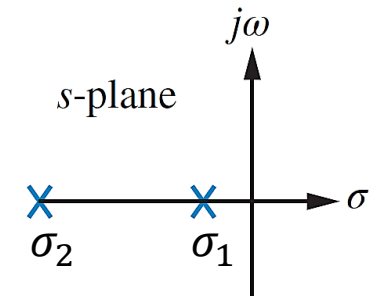


- Unlike first-order systems, changes in the parameters ( $a, b$ ) of a second-order system can totally change the **form** of the response. Therefore, depending on the location of two poles of the second-order system, it can exhibit different types of responses: **Overdamped**, **Underdamped**, **Undamped**, and **Critically Damped**.

# Unit-Step Response

## 1. Overdamped Response

When  $G(s)$  has two real poles at  $\sigma_1$  and  $\sigma_2$ :



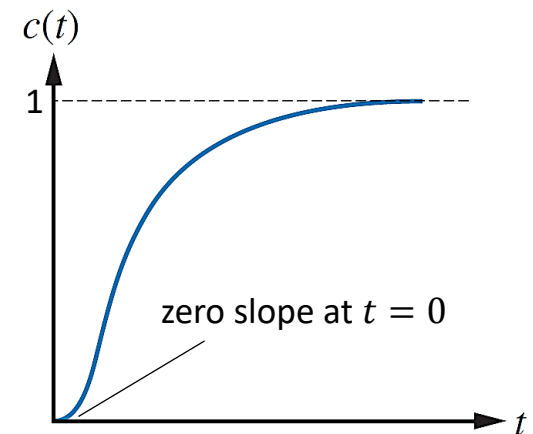
$$C(s) = R(s)G(s)$$

$$C(s) = \frac{1}{s} \cdot \frac{b}{s^2 + as + b} = \frac{1}{s} \cdot \frac{b}{(s + \sigma_1)(s + \sigma_2)}$$

$$= \frac{K_0}{s} + \frac{K_1}{s + \sigma_1} + \frac{K_2}{s + \sigma_2}$$

$$\begin{cases} \sigma_1 + \sigma_2 = a \\ \sigma_1\sigma_2 = b \end{cases}$$

$$c(t) = c_f(t) + c_n(t) = 1 + K_1 e^{-\sigma_1 t} + K_2 e^{-\sigma_2 t}$$



- It is called overdamped due to absorption of a large amount of energy in the system.

# Unit-Step Response

## 2. Underdamped Response

When  $G(s)$  has two complex poles at  $-\sigma_d \pm j\omega_d$ :

$$C(s) = R(s)G(s)$$

$$C(s) = \frac{1}{s} \cdot \frac{b}{s^2 + as + b} = \frac{K_0}{s} + \frac{K_1(s + \sigma_d) + K_2\omega_d}{(s + \sigma_d)^2 + \omega_d^2}$$

$$c(t) = c_f(t) + c_n(t) \quad \begin{cases} \sigma_d = a/2 \\ \omega_d^2 = b - (a/2)^2 \end{cases}$$

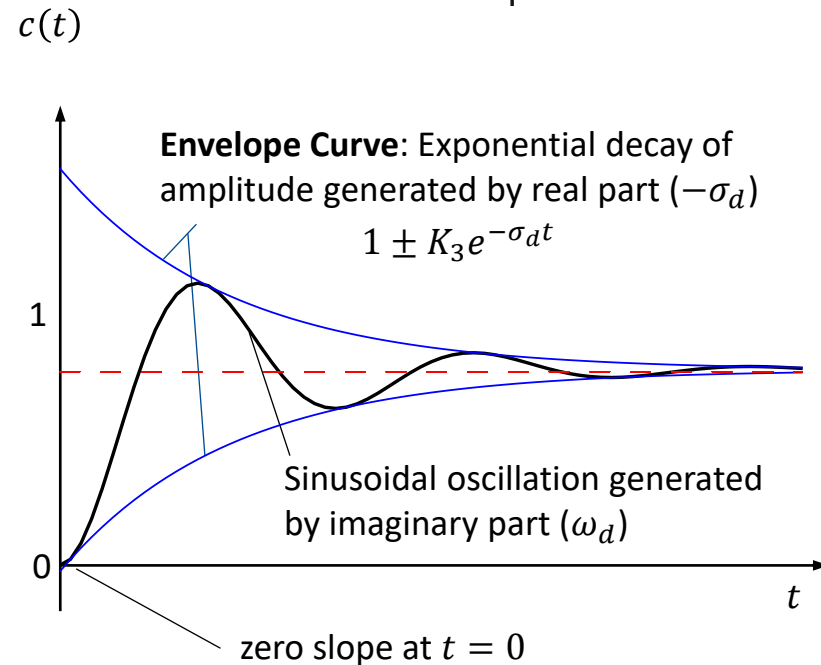
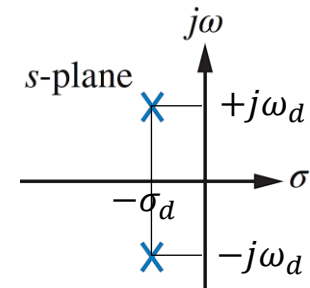
$$= 1 + e^{-\sigma_d t} (K_1 \cos \omega_d t + K_2 \sin \omega_d t)$$

$$= 1 + K_3 e^{-\sigma_d t} \cos(\omega_d t - \phi)$$

$$= 1 + K_3 e^{-\sigma_d t} \sin(\omega_d t + \bar{\phi})$$

$$\left( K_3 = \sqrt{K_1^2 + K_2^2}, \phi = \tan^{-1} \frac{K_2}{K_1}, \bar{\phi} = \tan^{-1} \frac{K_1}{K_2} \right)$$

- This is an exponentially damped sinusoidal response.



# Unit-Step Response

## 3. Undamped Response

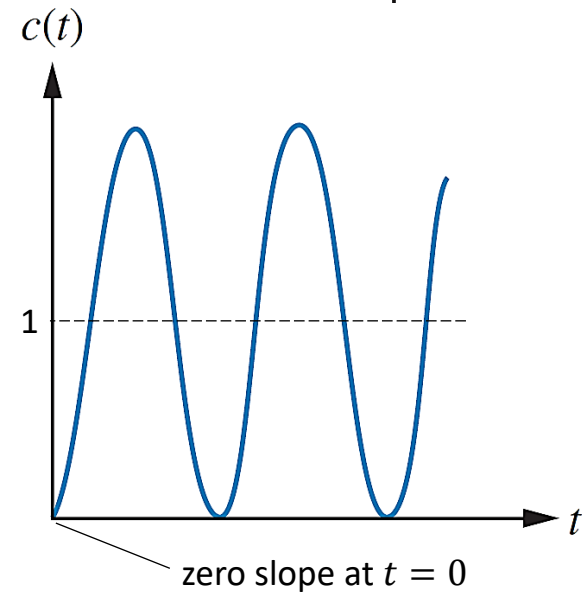
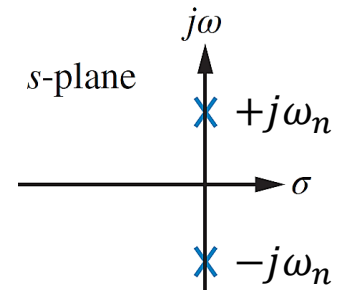
When  $G(s)$  has two imaginary poles at  $\pm j\omega_n$ :

$$C(s) = R(s)G(s)$$

$$C(s) = \frac{1}{s} \cdot \frac{b}{s^2 + as + b} = \frac{K_0}{s} + \frac{K_1s + K_2\omega_n}{s^2 + \omega_n^2} \quad \begin{cases} a = 0 \\ \omega_n^2 = b \end{cases}$$

$$\begin{aligned} c(t) &= c_f(t) + c_n(t) = 1 + K_1 \cos \omega_n t + K_2 \sin \omega_n t \\ &= 1 + K_3 \cos(\omega_n t - \phi) = 1 + K_3 \sin(\omega_n t + \bar{\phi}) \end{aligned}$$

$$\left( K_3 = \sqrt{K_1^2 + K_2^2}, \phi = \tan^{-1} \frac{K_1}{K_2}, \bar{\phi} = \tan^{-1} \frac{K_2}{K_1} \right)$$

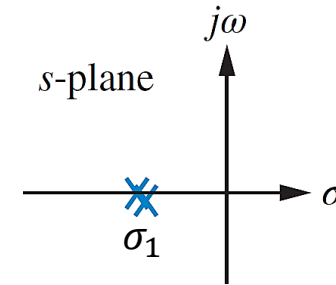


- This is a sinusoidal response whose frequency is  $\omega_n$  (i.e., location of the imaginary poles).

# Unit-Step Response

## 4. Critically-Damped Response

When  $G(s)$  has two repeated real poles at  $\sigma_1$ :



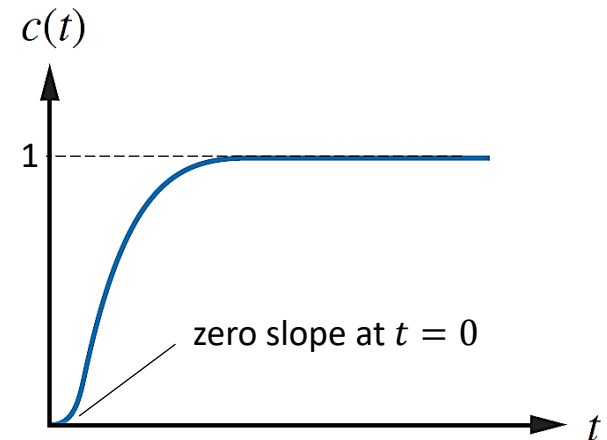
$$C(s) = R(s)G(s)$$

$$C(s) = \frac{1}{s} \cdot \frac{b}{s^2 + as + b} = \frac{1}{s} \cdot \frac{b}{(s + \sigma_1)^2}$$

$$= \frac{K_0}{s} + \frac{K_1}{(s + \sigma_1)} + \frac{K_2}{(s + \sigma_1)^2}$$

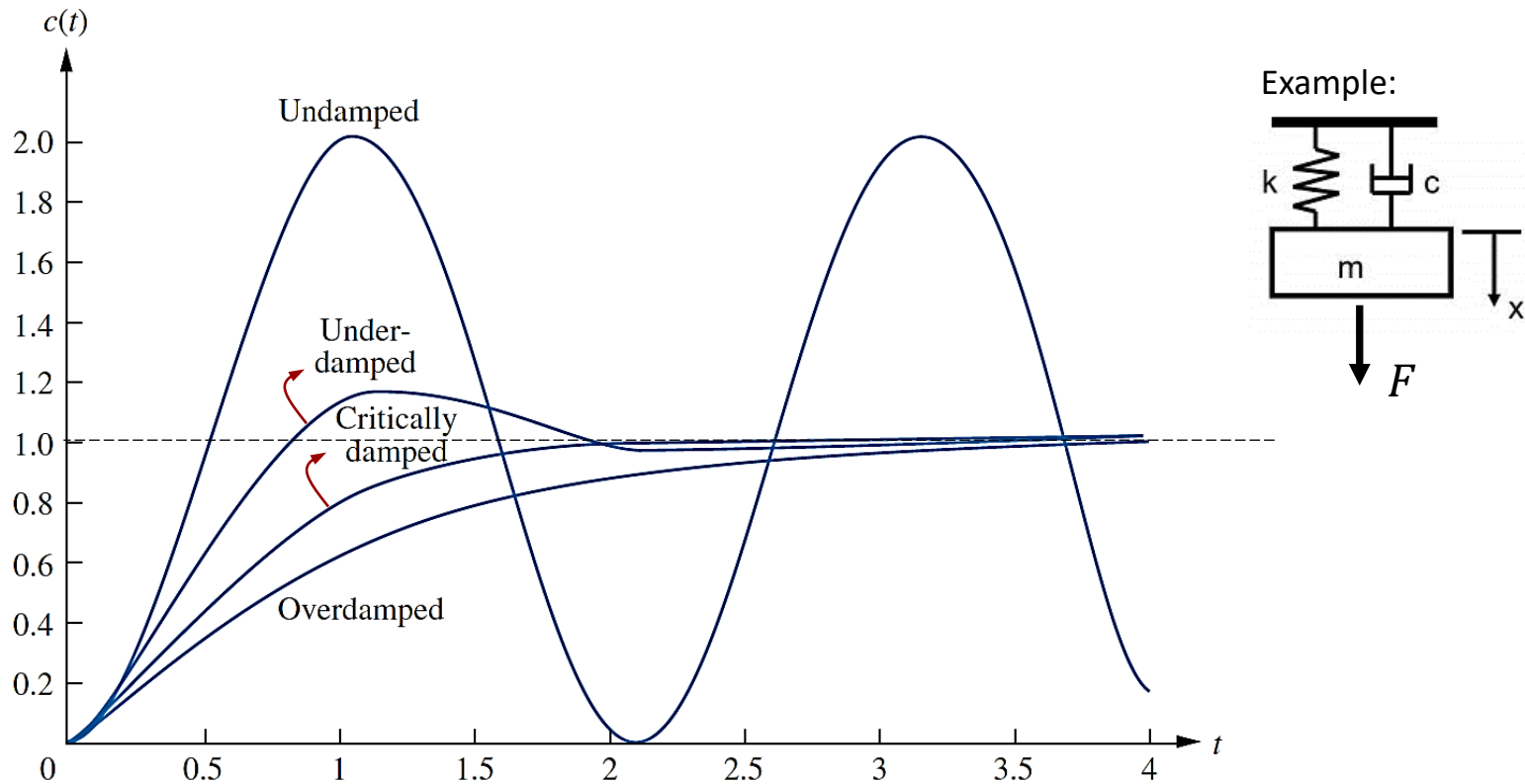
$$\begin{cases} 2\sigma_1 = a \\ \sigma_1^2 = b \end{cases}$$

$$c(t) = c_f(t) + c_n(t) = 1 + K_1 e^{-\sigma_1 t} + K_2 t e^{-\sigma_1 t}$$





# Unit-Step Response: Summary



- ❖ **Note:** The **critically damped** case is the division between the **overdamped** cases and the **underdamped** cases and is the **fastest response possible without overshoot**.

# A New Definition of Second-Order Systems

Two physically meaningful specifications/parameters used to describe the characteristics of the second-order transient response:

- **Natural Frequency** ( $\omega_n$ ): It is the frequency of system oscillation without damping.

$$G(s) = \frac{b}{s^2 + as + b} \quad \text{Without damping, the poles would be on the } j\omega\text{-axis} \rightarrow a = 0 \rightarrow \omega_n = \sqrt{b}$$

- **Damping Ratio** ( $\zeta$ ):  $\zeta = \frac{\text{Exponential decay frequency}}{\text{Natural frequency (rad/s)}} \rightarrow \zeta = \frac{\sigma_d}{\omega_n} = \frac{a/2}{\omega_n} = \frac{a}{2\sqrt{b}}$

$$\Rightarrow \begin{cases} b = \omega_n^2 \\ a = 2\zeta\omega_n \end{cases}$$

Therefore, standard form of a second-order system in terms of  $\zeta$  and  $\omega_n$  can be written as

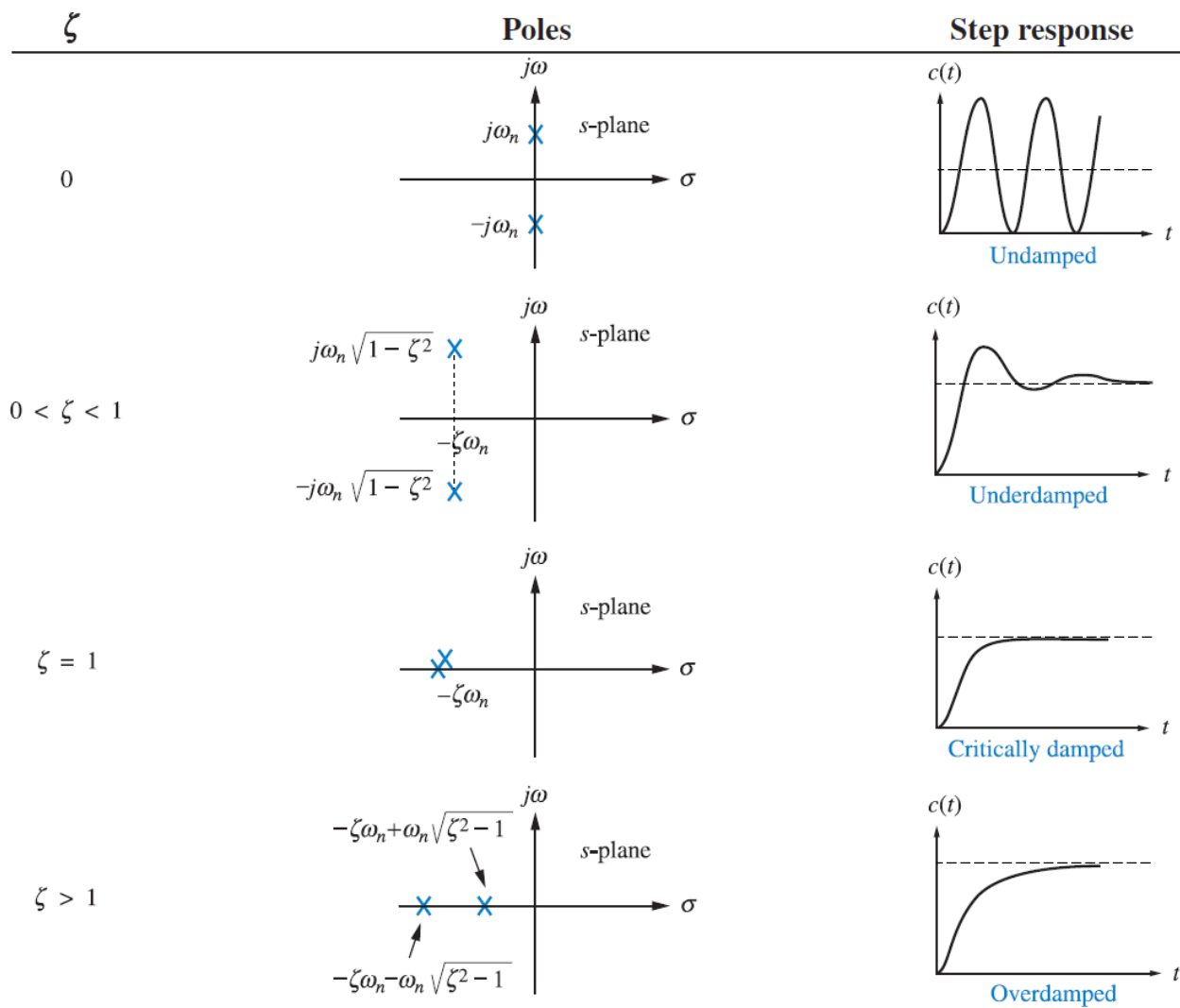
$$G(s) = \frac{b}{s^2 + as + b} \rightarrow G(s) = \frac{\omega_n^2}{s^2 + 2\zeta\omega_n s + \omega_n^2} \quad \text{Poles: } -\zeta\omega_n \pm \omega_n\sqrt{\zeta^2 - 1}$$

# Step Response of Second-Order Systems Using the New Definition

The step response can be classified based on the value of  $\zeta$ :

$$G(s) = \frac{\omega_n^2}{s^2 + 2\zeta\omega_n s + \omega_n^2}$$

Poles:  $-\zeta\omega_n \pm \omega_n\sqrt{\zeta^2 - 1}$



# Example

For the given the transfer function, find  $\zeta$  and  $\omega_n$ .

$$G(s) = \frac{360}{s^2 + 4.2s + 36}$$

**Answer:**  $\omega_n = 6$ ,  $\zeta = 0.35$

# Underdamped Second-Order Systems

# Step Response of Underdamped Second-Order Systems

Underdamped second-order systems (i.e., when  $0 < \zeta < 1$ ) are common in physical problems. Thus, a detailed description of these systems is necessary for both analysis and design.

$$C(s) = R(s)G(s) = \frac{1}{s} \cdot \frac{\omega_n^2}{s^2 + 2\zeta\omega_n s + \omega_n^2} = \frac{K_1}{s} + \frac{K_2 s + K_3}{s^2 + 2\zeta\omega_n s + \omega_n^2}$$

$$c(t) = 1 - e^{-\sigma_d t} \left( \cos \omega_d t + \frac{\zeta}{\sqrt{1 - \zeta^2}} \sin \omega_d t \right) = 1 - \frac{e^{-\sigma_d t}}{\sqrt{1 - \zeta^2}} \cos(\omega_d t - \phi)$$

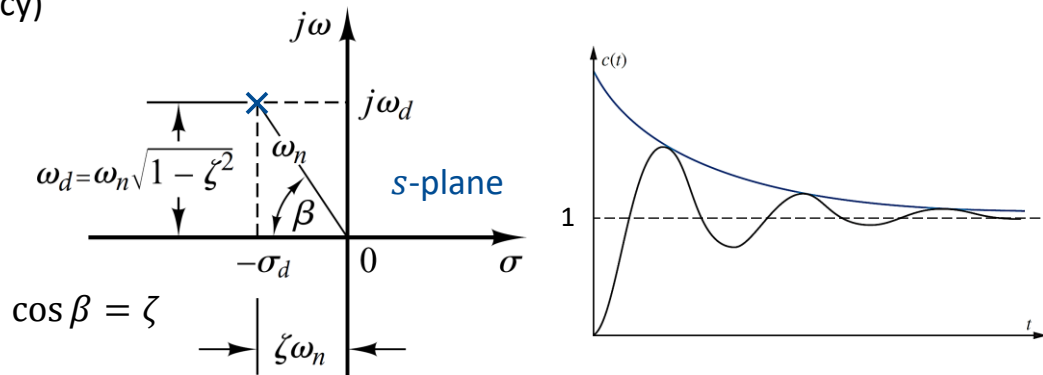
$$= 1 - \frac{e^{-\sigma_d t}}{\sqrt{1 - \zeta^2}} \sin(\omega_d t + \bar{\phi})$$

$\sigma_d = \zeta\omega_n$  (Exponential Damping Frequency or Attenuation)

$\omega_d = \omega_n\sqrt{1 - \zeta^2}$  (Damped Natural Frequency)

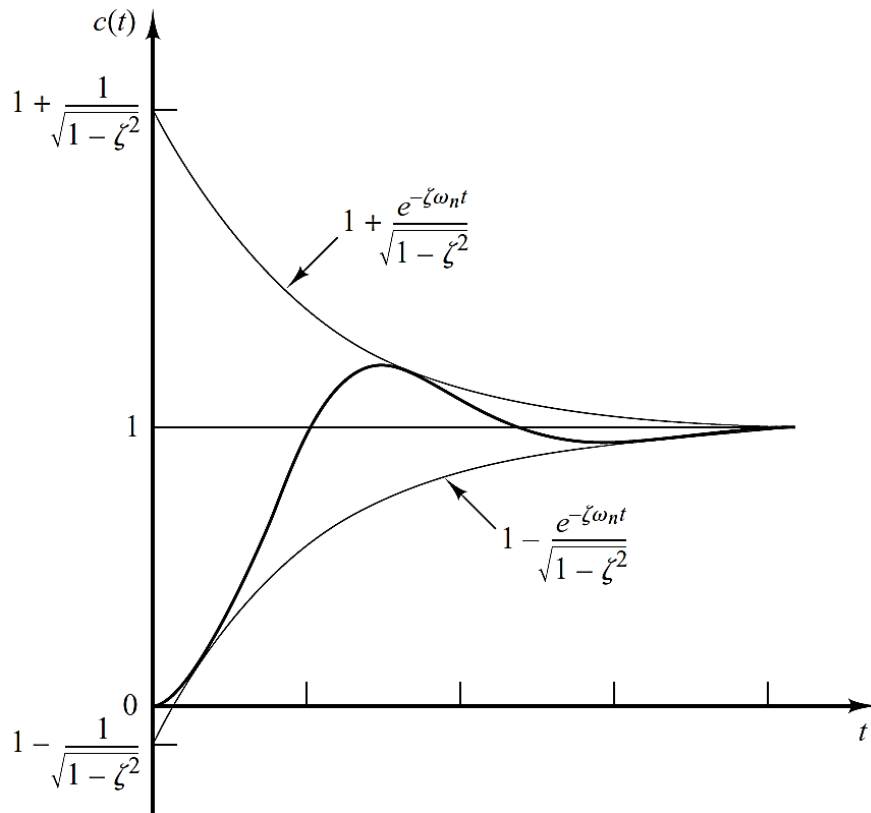
$\phi = \tan^{-1}(\zeta/\sqrt{1 - \zeta^2})$

$\bar{\phi} = \tan^{-1}(\sqrt{1 - \zeta^2}/\zeta)$

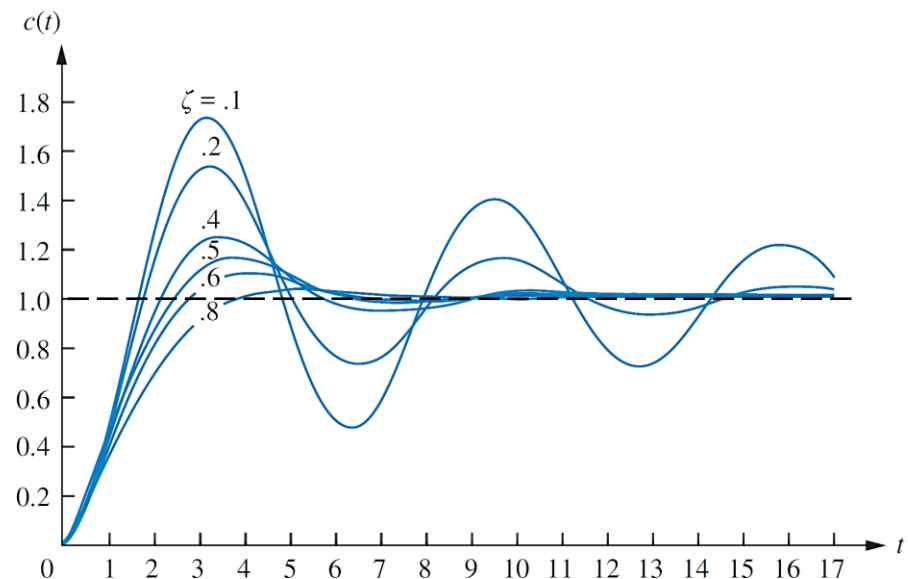


# Step Response of Underdamped Second-Order Systems

Pair of envelope curves for the unit-step response:



Unit-step response for different damping ratio  $\zeta$  values:



# Parameters of Step Response of Underdamped Second-Order Systems

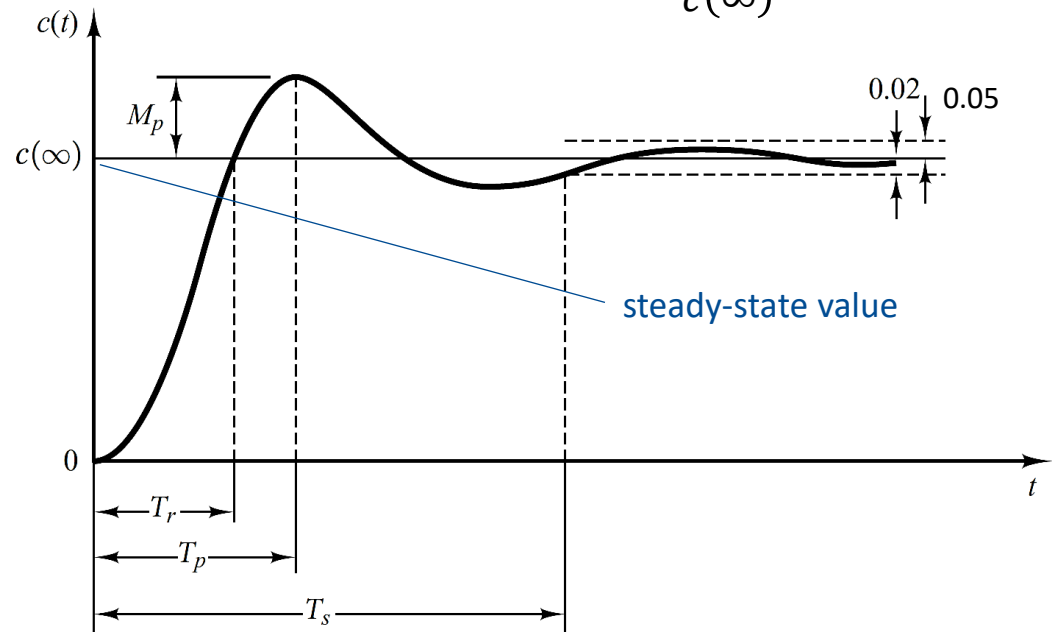
The parameters defined for the step input response of underdamped second-order systems:

1. **Peak Time**  $T_p$ : The time required for the response to reach the **first** (or maximum) peak.
2. **Maximum Overshoot**  $M_p$ : The percentage of the steady-state value that the response overshoots the steady-state value at the peak time  $T_p$ .

$$M_p = \frac{c(T_p) - c(\infty)}{c(\infty)} \times 100$$

3. **Settling Time**  $T_s$ : The time required for the response to **reach and stay** within 2% (or 5%) of the steady-state value.

4. **Rise Time**  $T_r$ : The time required for the response to go from 0% to 100% (or 10% to 90% or 5% to 95%) of the steady-state value.





# Calculation of Parameters: $T_p$

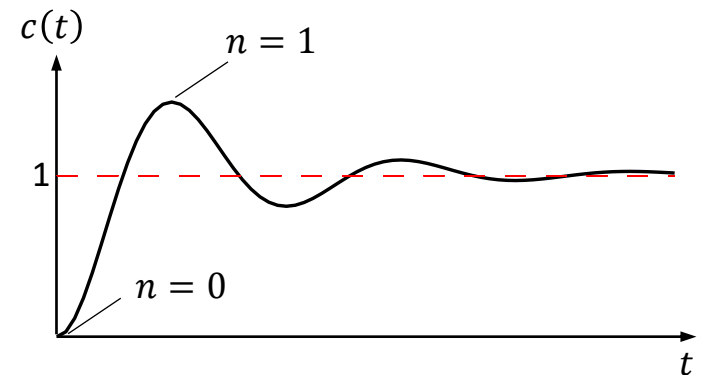
**Peak Time  $T_p$ :**

$$T_p = t \Big|_{\dot{c}(t)=0} \Rightarrow \dot{c}(t) = \frac{d \left( 1 - e^{-\sigma_d t} \left( \cos \omega_d t + \frac{\zeta}{\sqrt{1-\zeta^2}} \sin \omega_d t \right) \right)}{dt} = 0 \Rightarrow$$

$$\dot{c}(t) = \frac{\omega_n}{\sqrt{1-\zeta^2}} e^{-\sigma_d t} \sin \omega_d t = 0 \Rightarrow \omega_d t = n\pi$$

Each value of  $n$  yields the time for local maxima or minima. Letting  $n = 0$  yields  $t = 0$ . The first peak is found by letting  $n = 1$ :

$$T_p = \frac{\pi}{\omega_d}$$



# Calculation of Parameters: $M_p$

**Maximum Overshoot  $M_p$ :**

$$M_p = \frac{c(T_p) - c(\infty)}{c(\infty)} \times 100$$

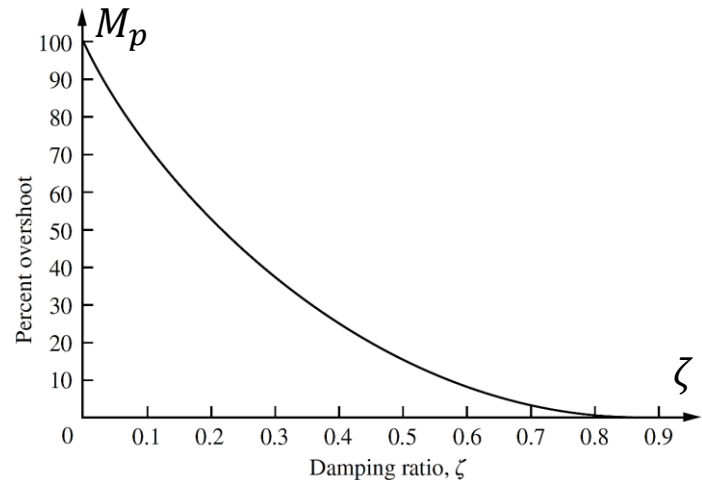
$$c(T_p) = c\left(\frac{\pi}{\omega_d}\right) = 1 - e^{-\sigma_d \pi / \omega_d} \left( \cos \pi + \frac{\zeta}{\sqrt{1-\zeta^2}} \sin \pi \right) = 1 + e^{-(\zeta \pi / \sqrt{1-\zeta^2})}$$

$$c(\infty) = 1 \quad (\text{For the unit step})$$

$$M_p = e^{-(\zeta \pi / \sqrt{1-\zeta^2})} \times 100$$

(or)

$$\zeta = \frac{-\ln(M_p/100)}{\sqrt{\pi^2 + \ln^2(M_p/100)}}$$



# Calculation of Parameters: $T_s$

## Settling Time $T_s$ :

We can find  $T_s$  by finding the time it takes for the envelope curve to reach 2% or 5% of the steady-state value.

- For 2% of the steady-state value:

$$1 - \left(1 - \frac{e^{-\sigma_d t}}{\sqrt{1 - \zeta^2}}\right) = 0.02 \quad \Rightarrow \quad \frac{e^{-\sigma_d t}}{\sqrt{1 - \zeta^2}} = 0.02$$

$$\Rightarrow T_s = \frac{-\ln(0.02\sqrt{1 - \zeta^2})}{\sigma_d}$$

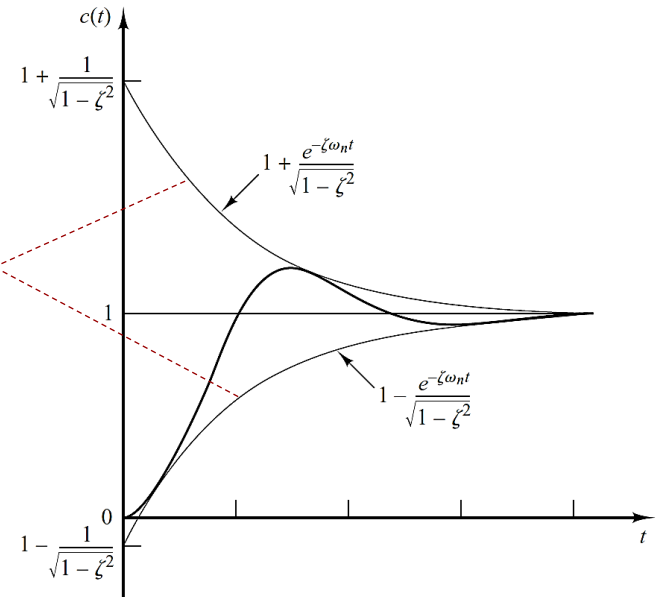
Since for  $0 < \zeta < 0.9$ , we have

$$3.91 < -\ln(0.02\sqrt{1 - \zeta^2}) < 4.74$$

$$\Rightarrow T_s \approx \frac{4}{\sigma_d}$$

- Similarly, for 5% of the steady-state value:

$$T_s \approx \frac{3}{\sigma_d}$$



# Calculation of Parameters: $T_r$

## Rise Time $T_r$ :

- For 10% to 90%, a precise analytical relationship cannot be found.
- For 0% to 100%:

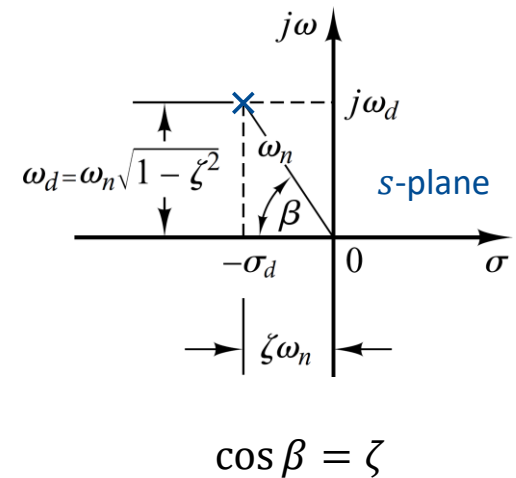
$$T_r = t \Big|_{c(t)=c(\infty)} - t \Big|_{c(t)=0} \Rightarrow c(T_r) = 1 \Rightarrow$$

$$1 - e^{-\sigma_d T_r} \left( \cos \omega_d T_r + \frac{\zeta}{\sqrt{1-\zeta^2}} \sin \omega_d T_r \right) = 1 \Rightarrow$$

$$\cos \omega_d T_r + \frac{\zeta}{\sqrt{1-\zeta^2}} \sin \omega_d T_r = 0 \Rightarrow$$

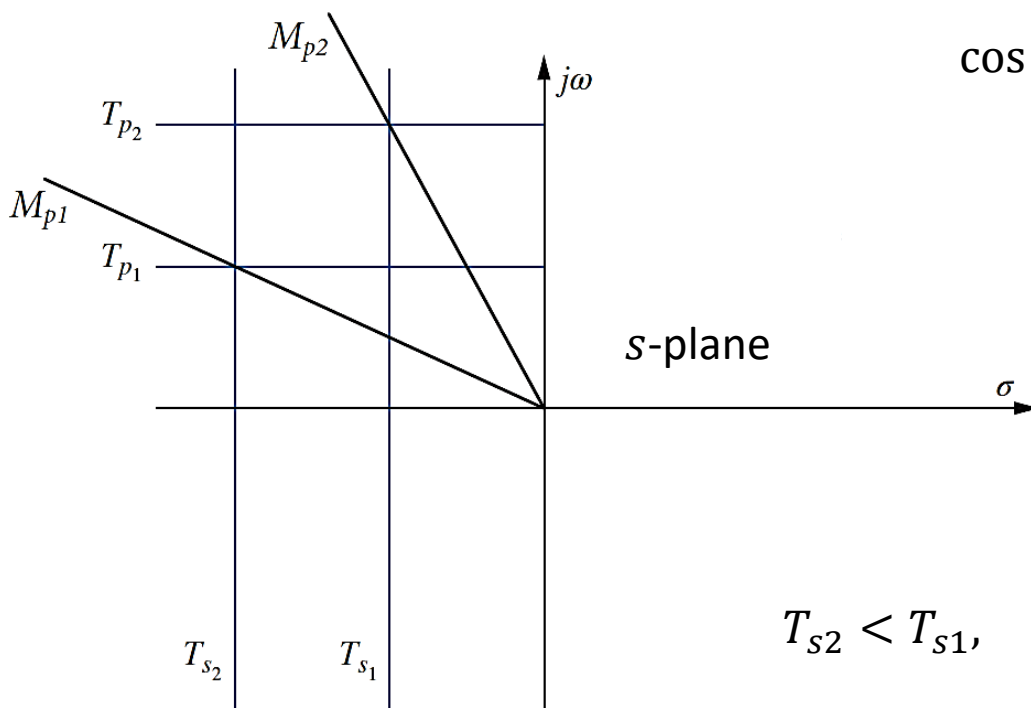
$$T_r = \frac{1}{\omega_d} \tan^{-1} \left( \frac{\sqrt{1-\zeta^2}}{-\zeta} \right) = \frac{1}{\omega_d} \tan^{-1} \left( \frac{\omega_d}{-\sigma_d} \right) = \frac{\pi - \beta}{\omega_d}$$

(from above figure)



# Lines of Constant $T_s$ , $T_p$ , and $M_p$

- **Vertical** lines on the  $s$ -plane are lines of constant **Settling Time**, since  $T_s = 4/\sigma_d$ .
- **Horizontal** lines on the  $s$ -plane are lines of constant **Peak Time**, since  $T_p = \pi/\omega_d$ .
- **Radial** lines on the  $s$ -plane are lines of constant  $\zeta$  and **Maximum Overshoot**, since



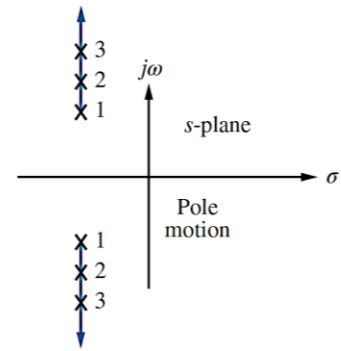
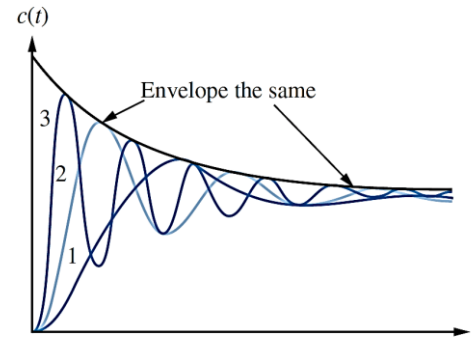
$$\cos \beta = \zeta, \quad M_p = e^{-\left(\zeta\pi/\sqrt{1-\zeta^2}\right)} \times 100$$

$$T_{s2} < T_{s1}, \quad T_{p2} < T_{p1}, \quad M_{p1} < M_{p2}$$

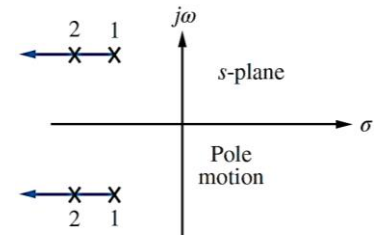
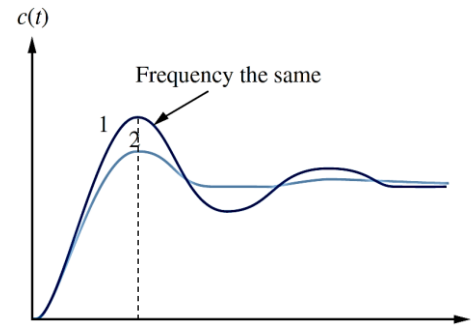
# Step Responses of Underdamped 2nd-Order Systems as Poles Move

$$T_r = (\pi - \beta)/\omega_d, T_p = \pi/\omega_d, T_s = 4/\sigma_d, \cos \beta = \zeta$$

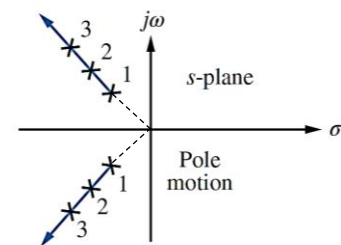
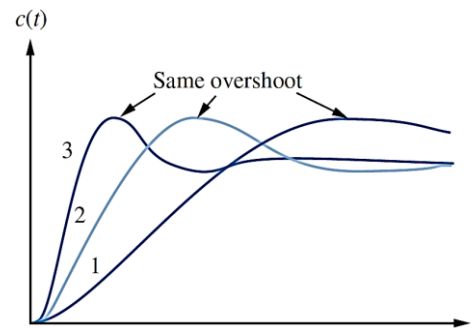
As the poles move in a vertical direction upward,  $\omega_d$  and  $M_p$  increase,  $T_p$  and  $T_r$  decrease, and  $T_s$  remains constant.



As the poles move in a horizontal direction to the left,  $M_p$  and  $T_s$  decrease (the response damps out more rapidly),  $T_r$  increases,  $\omega_d$  and  $T_p$  remain constant.



As the poles move diagonally away from the origin,  $\omega_d$  increases,  $T_r$ ,  $T_s$ , and  $T_p$  decrease, and  $M_p$  remains constant.

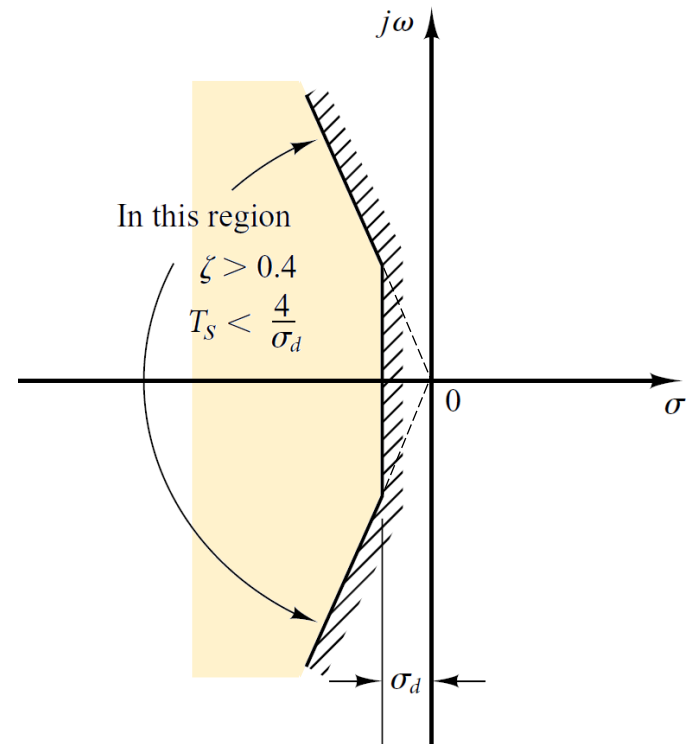


# Some Comments

- Except for certain applications where oscillations cannot be tolerated, it is desirable that the transient response be sufficiently fast and be sufficiently damped. Thus, for a **desirable transient response** of a second-order system, the damping ratio ( $\zeta$ ) must be **between 0.4 and 0.8**. Values of  $\zeta < 0.4$  yield excessive overshoot and values of  $\zeta > 0.8$  responds slowly.

- To guarantee specific, desired transient response characteristics, it is necessary that the poles of the system lie in a particular region in the complex plane.

For example, in this figure, a desired region for poles of a 2<sup>nd</sup>-order system to have fast ( $T_s < 4/\sigma$ ), yet well-damped ( $\zeta > 0.4$ ), transient response characteristics, is shown.



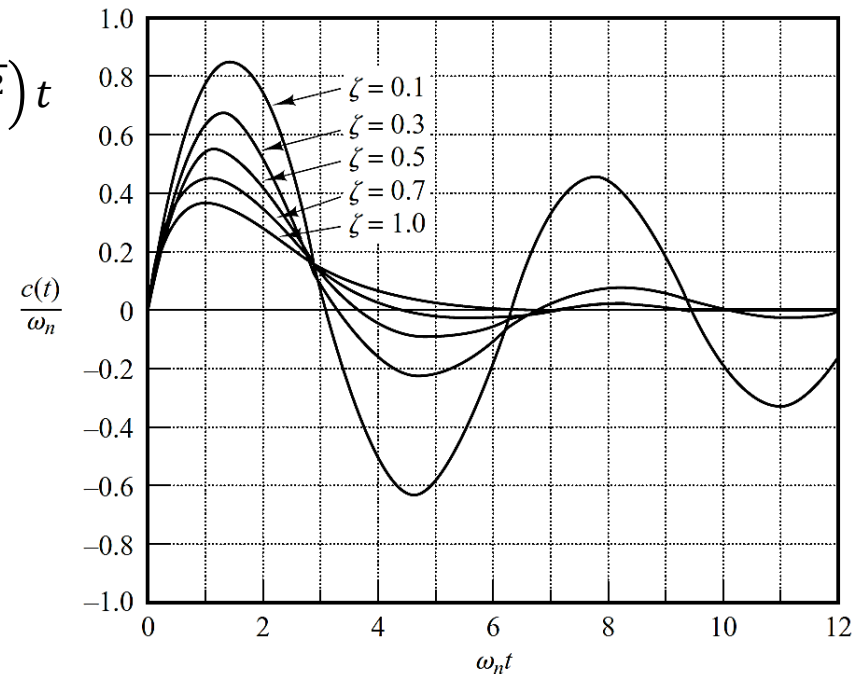
# Impulse Response of Second-Order Systems

**Impulse Response** of second-order systems can be derived by **differentiating** the corresponding unit-step response, since the unit-impulse function is the time derivative of the unit-step function.

- $0 \leq \zeta < 1$ : 
$$c(t) = \frac{\omega_n}{\sqrt{1 - \zeta^2}} e^{-\zeta\omega_n t} \sin\left(\omega_n \sqrt{1 - \zeta^2}\right) t$$

- $\zeta = 1$ : 
$$c(t) = \omega_n^2 t e^{-\omega_n t}$$

- $\zeta > 1$ : 
$$c(t) = \frac{\omega_n}{2\sqrt{\zeta^2 - 1}} e^{-(\zeta - \sqrt{\zeta^2 - 1})\omega_n t} - \frac{\omega_n}{2\sqrt{\zeta^2 - 1}} e^{-(\zeta + \sqrt{\zeta^2 - 1})\omega_n t}$$



**Note:**

$$\ddot{x} + a\dot{x} + bx = b\delta(t),$$

$$x(0^-) = 0, \dot{x}(0^-) = 0$$



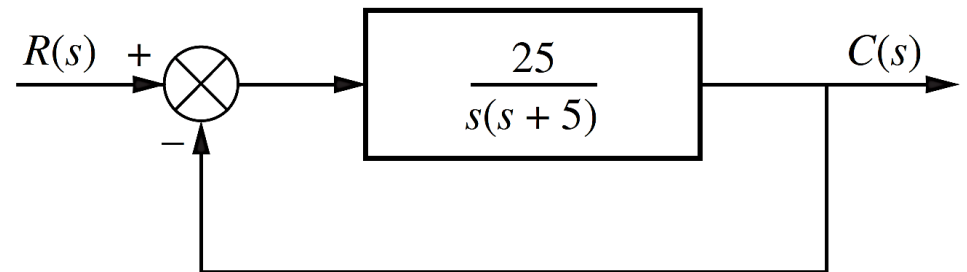
$$\ddot{w} + a\dot{w} + bw = 0,$$

$$\dot{w}(0^+) = b, w(0^+) = 0$$



# Example

Find the peak time, maximum overshoot, and settling time (to reach 2% of the steady-state value).

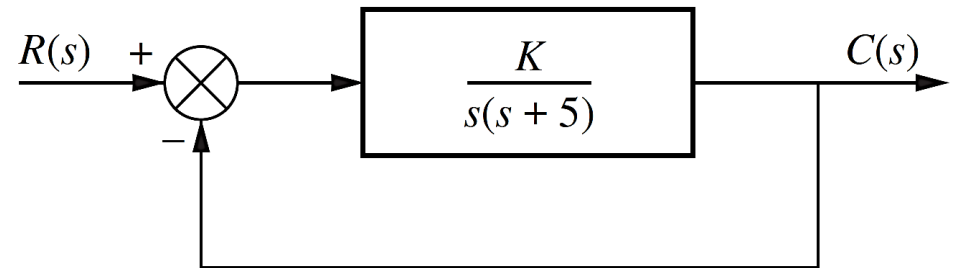


**Answer:**

$$T_p = 0.726 \text{ s}, \quad M_p = 16.303, \quad T_s = 1.6 \text{ s}$$

# Example

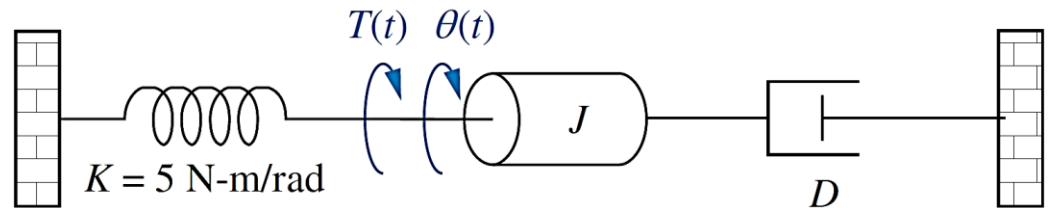
Design the value of gain  $K$  for the shown feedback control system so that the system will respond to a step input with a 10% overshoot.



**Answer:**  $K = 17.9$

# Example

Given the system shown, find  $J$  and  $D$  to yield 20% overshoot and a settling time of 2 seconds for a step input of torque  $T(t)$ .



**Answer:**

$$J = 0.26 \text{ kgm}^2 \quad D = 1.04 \text{ Nms/rad}$$

# Using MATLAB and Control System Toolbox

# Time Response of Systems Using step and impulse

## For Unit-Step Response:

```
num = 4;  
den = [1 1 4];  
T1 = tf(num,den);
```

```
% Unit-Step Response  
step(T1)
```

```
% Unit-Step Response for a given time range  
figure  
t_range = 0:0.1:15;  
step(T1,t_range)
```

```
% or  
figure  
[y,t] = step(T1);  
plot(t,y)
```

```
% Time response of multiple systems
```

```
T2 = tf(1,[1 2 1]);  
T3 = tf(4,[1 4 4]);  
T4 = tf(4,[1 1 4]);
```

```
figure  
step(T2,T3,T4)
```

```
% or  
figure  
step(T2,'r-',T3,'k-.',T4,'b--')
```

- When  $t$  is not explicitly included in the step commands, the time vector is automatically determined.

## For Unit-Impulse Response:

**Method 1:** Substitute the command "step" with command "impulse".

**Method 2:** The unit-impulse response of  $G(s)$  is the same as the unit-step response of  $sG(s)$ .

# Time Response of Systems Using Isim

## For Unit-Ramp Response:

**Method 1:** The unit-ramp response of  $G(s)$  is the same as the unit-step response of  $G(s)/s$ .

**Method 2:** Use the general command "lsim".

```
lsim(sys,r,t)  
y = lsim(sys,r,t)
```

The command "lsim" is used to obtain the response to an **arbitrary input**.

```
num = 4;  
den = [1 1 4];  
T1 = tf(num,den);  
t = 0:0.1:10;  
r = t; % ramp input  
y = lsim(T1,r,t);  
figure  
plot(t,r,'-!',t,y,'-!')
```

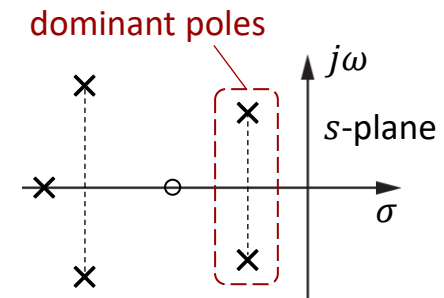
To find step-response characteristics (e.g.,  $T_p$ ,  $T_s$ , ...) use stepinfo.

```
stepinfo(sys)
```

# Higher-Order Systems

# Dominant Poles

- If a system has more than two poles or has zeros, **analytical** expressions for  $T_s$ ,  $T_p$ , and  $M_p$  cannot be found and the transient response of these systems to any given input can be obtained by a **computer simulation**. However,
  - If the system has just two **complex dominant poles**, it can be approximated as a **second-order system** and all the derived formulas for  $T_s$ ,  $T_p$ , and  $M_p$  of the second-order systems can be used.
  - Transient response of all other higher-order systems can be considered using **Root Locus** techniques (that will be covered in the next chapters).
- In this section, the effect of **adding a pole** to a second-order system  $T(s)$  is investigated.



$$T'(s) = \frac{T(s)}{(s + p_3)} = \frac{k}{(s^2 + as + b)(s + p_3)}$$

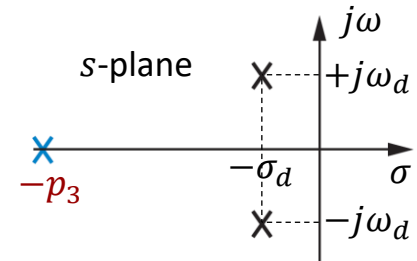


# System Response with an Additional Pole

Consider the unit-step response of a three-pole system  $T'(s)$  with two complex dominant poles  $-\sigma_d \pm j\omega_d$  and a real pole  $p_3$ :

$$C(s) = \frac{1}{s} \cdot \frac{k}{(s^2 + as + b)(s + p_3)} = \frac{K_1}{s} + \frac{K_2(s + \sigma_d) + K_3\omega_d}{(s + \sigma_d) + \omega_d^2} + \frac{K_4}{s + p_3}$$

$$c(t) = K_1 + e^{-\sigma_d t} (K_2 \cos \omega_d t + K_3 \sin \omega_d t) + K_4 e^{-p_3 t}$$

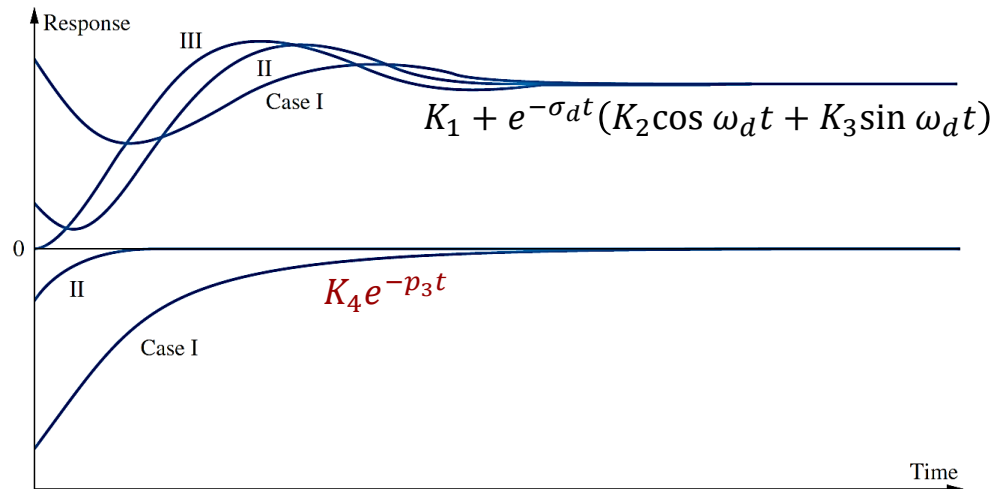


Comparison of the component parts of  $c(t)$  for 3 cases:

**Case I:**  $p$  is near dominant complex dominant poles (i.e.,  $p_3 > \sigma_d$ ).

**Case II:**  $p$  is far from dominant complex dominant poles (i.e.,  $p_3 \gg \sigma_d$ ).

**Case III:**  $p$  is at infinity (i.e.,  $p_3 = \infty$ , and consequently,  $K_4 = 0$ ).



# System Response with an Additional Pole

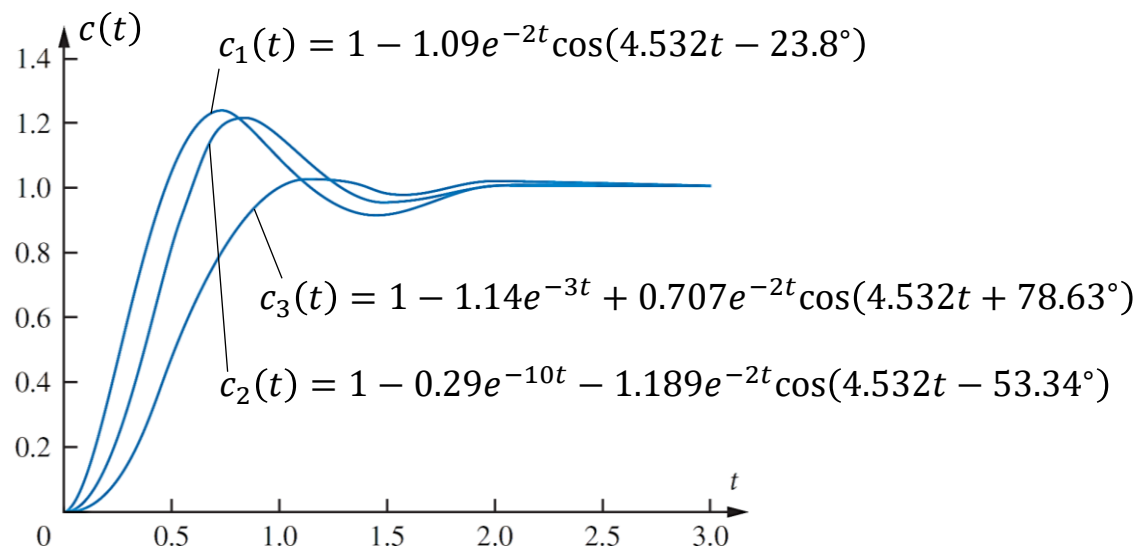
Therefore, if the term  $K_4 e^{-p_3 t}$  decays to an insignificant value at the time of the first overshoot, then  $T_s$ ,  $T_p$ , and  $M_p$  will be generated by the underdamped second-order step response component and the system can be represented as a **pure second-order system**.

**Example:**

$$T_1(s) = \frac{24.542}{s^2 + 4s + 24.542}$$

$$T_2(s) = \frac{245.42}{(s + 10)(s^2 + 4s + 24.542)}$$

$$T_3(s) = \frac{73.626}{(s + 3)(s^2 + 4s + 24.542)}$$



**Note:** It can be assumed that if the real pole  $p_3$  is **five times** farther to the left than the dominant poles (i.e.,  $p_3 > 5\sigma_d$ ), the system is represented by its dominant second-order pair of poles.

**Note:** The magnitude of residue of the non-dominant pole ( $K_4$ ) will also decrease as the pole is moved farther into the left of  $j\omega$ -axis.

# Example

Determine the validity of a second-order approximation for each of these two transfer functions:

$$\text{a) } G(s) = \frac{700}{(s + 15)(s^2 + 4s + 100)}$$

$$\text{b) } G(s) = \frac{360}{(s + 4)(s^2 + 2s + 90)}$$

**Answer:** a) Valid, b) invalid

# Systems with Zeros

# System Response with a Zero

Let  $C(s)$  be the response of a system  $T(s)$ , with a constant in the numerator. If we add a zero to the transfer function, i.e.,  $T'(s) = (s + z)T(s)$ , the **response** will consist of **two parts**:

$$C'(s) = (s + z)C(s) = sC(s) + zC(s)$$

$$c'(t) = \dot{c}(t) + zc(t)$$

(Derivative of the  
original response)

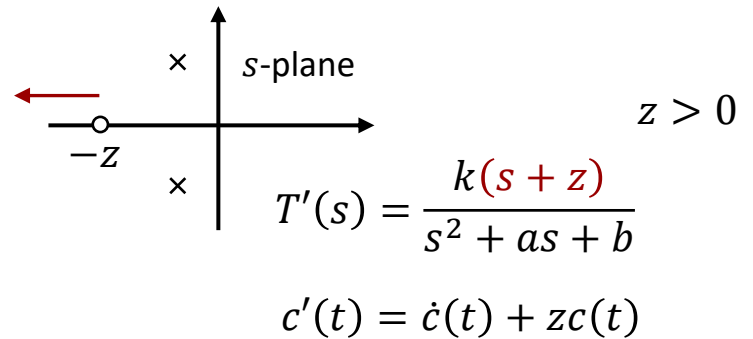
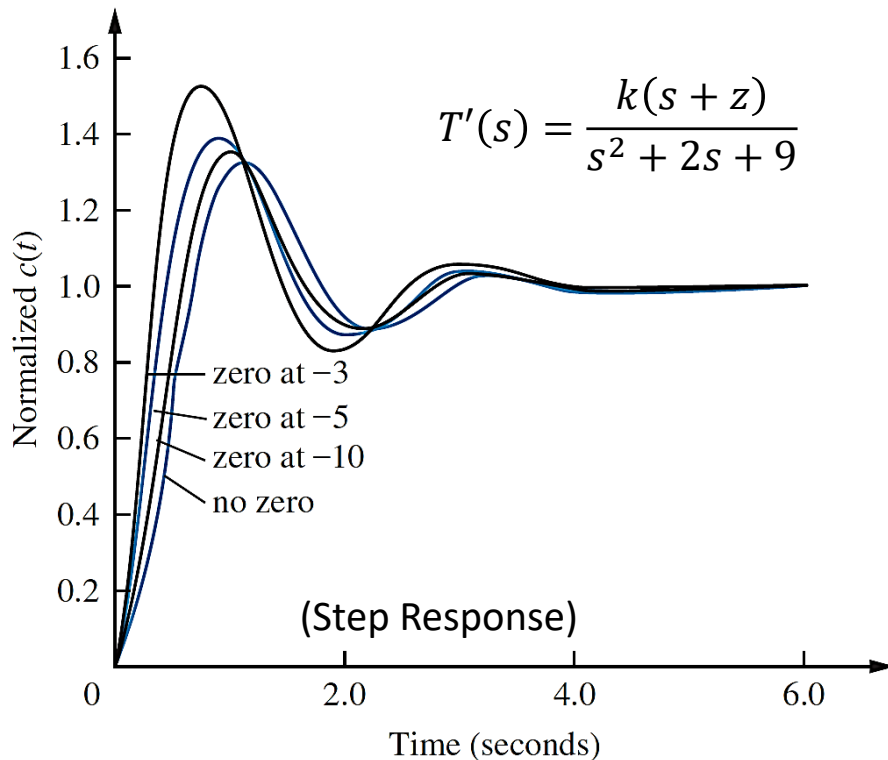
(A scaled version of  
the original response)

- In this section, the effect of **adding a zero** to a second-order system  $T(s)$  is investigated.

$$T'(s) = T(s)(s + z) = \frac{k(s + z)}{s^2 + as + b}$$

# System Response with a Negative Zero

Let  $T'(s)$  be a second-order system with a **negative real zero**  $z$  (i.e.,  $z$  is placed in the **Left Half-Plane** or **LHP**). As the  $z$  moves away from the dominant poles to the left, the derivative term  $\dot{c}(t)$  contributes less to the response  $c'(t)$  and the response approaches to the form of the second-order system and the zero acts as a simple gain factor (i.e.,  $c'(t) \approx zc(t)$ ).

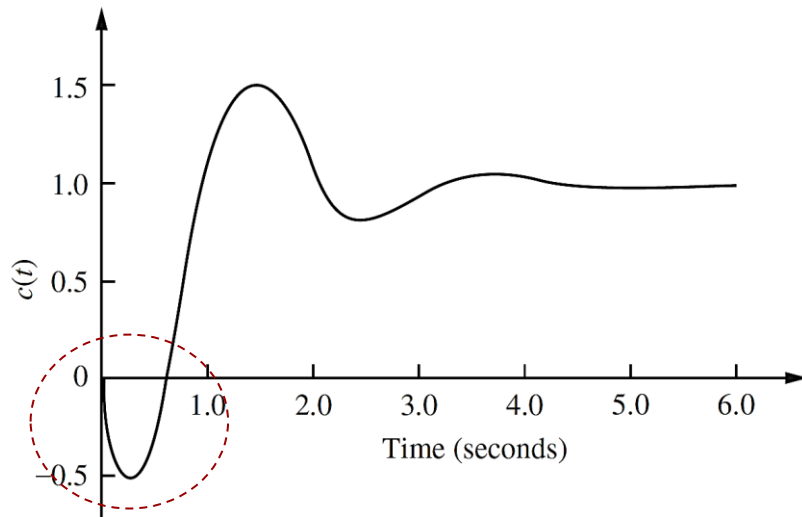


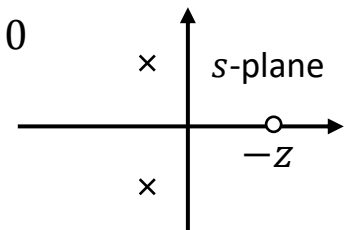
For step response,  $c(t) > 0$ ,  $\dot{c}(t) > 0$ ,  $zc(t) > 0$ , then  $c'(t) > 0$ .

- As  $z$  becomes smaller (closer to the dominant poles), the derivative term contributes more to the response and maximum overshoot increases.

# System Response with a Positive Zero (Minimum-Phase & Nonminimum-Phase Systems)

Let  $T'(s)$  be a second-order system with a **positive real zero**  $z$  (i.e.,  $z$  is placed in the **Right Half-Plane** or **RHP**). In this case, the step response first begins to turn toward the negative direction even though the steady-state value is positive.



$$T'(s) = \frac{k(s+z)}{s^2+as+b} \quad z < 0$$


s-plane

$$c'(t) = \dot{c}(t) + zc(t)$$

For step response,  $c(t) > 0$ ,  $\dot{c}(t) > 0$ , but since  $z < 0$ , then  $zc(t) < 0$ .

- ❖ If all the poles and zeros of a system lie in the LHP, then the system is called **Minimum Phase**. If a system has at least one pole or zero in the RHP, then the system is called **Non-Minimum-Phase (NMP)** phase.

# Pole-Zero Cancellation

Consider a three-pole system with a zero.

$$G(s) = \frac{k(s + z)}{(s^2 + as + b)(s + p_3)}$$

- If the pole term,  $(s + p_3)$ , and the zero term,  $(s + z)$ , cancel out (i.e.,  $z = p_3$ ), the system is **approximated as a second-order system**.
- If the zero at  $-z$  is **very close** to the pole at  $-p_3$  (i.e.,  $z \approx p_3$ ), then the amplitude of the exponential decay  $e^{-p_3 t}$  in the step-input response is much smaller than the other amplitudes and the system can be **approximated as a second-order system**. Hence, a pair of closely located poles and zeros will effectively cancel each other.

$$C(s) = \frac{1}{s} G(s) = \frac{0.87}{s} - \frac{5.3}{s+5} + \frac{4.4}{s+6} + \frac{0.033}{s+4.01} \quad \xrightarrow{\approx 0} \quad c_2(t) = 0.87 - 5.3e^{-5t} + 4.4e^{-6t} + 0.033e^{-4.01t} \quad \xrightarrow{\approx 0}$$

$$G(s) = \frac{26.25(s+4)}{(s+4.01)(s+5)(s+6)}$$